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APPLICATION FOR LETTERS PATENT

TITLE: TELECOMMUNICATION DEVICE WITH ANALOG
FOURIER TRANSFORMATION UNIT

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Description

- 1 The present invention relates to an OFDM telecommunication device, i. e. to
receivers, transmitters and transceivers for OFDM- (Orthogonal Frequency-
Division Multiplex) signals that generally employ the Inverse Fourier Trans-
formation (IFT) technique to encode and transmit time-division multiplex
5 signals and the Fourier Transformation (FT) technique to decode the received
signals into time-division multiplex signals.

A common OFDM receiver is shown in Fig. 8a. The OFDM-signal is received by
an antenna 100 and fed via an amplification and pre-processing circuit 101 as
10 RF- or n-IF-signal to a multiplier 102 that down-converts the received, ampli-
fied and pre-processed OFDM-signal into an IF-signal on basis of a demodula-
tion signal from an oscillator 103. This IF-signal is input to an IQ-demodulator
104 that additionally receives a demodulating signal from an oscillator 105
and produces the complex spectrum of the demodulated OFDM-signal, i. e. an
15 inphase signal I and a quadrature signal Q. These both signals are input to an
analog-to-digital converter 106 to leave the analog stage of the receiver and to
enter its digital stage wherein first a Fast Fourier Transformation is carried
out with a FFT-unit 107 before a demapper 108 produces a baseband signal
for the further processing. It can be seen that an FT-process is implemented
20 within the digital stage which therefore needs a relatively high processing
power.

As OFDM modulation schemes seem to be widely accepted for different public
broadcasting systems like DAB, DVB-T and private WLANs as a modulation
25 scheme the requirements in regard to the needed bandwidth increase and
therefore larger number of carriers are needed, which can be hardly handled
by one digital processor. Therefore, to cope with this coming situation, differ-
ent paralleling techniques have to be incorporated into future OFDM telecom-
munication devices. Such a block processing (parallel to serial conversion and
30 vice versa) means that a large amount of processing power might be necessary
and a large power consumption might arise as well as increased printed circuit
board layout requirements have to be thought of.

On the other hand, analog processing techniques to perform the Fourier
35 Transformation are known, e. g. from US 5,226,038 which discloses a method

1 and apparatus for converting electronic signals from frequency-division multi-
plex format into time-division multiplex format to perform an antenna beam
forming and thereafter to perform a conversion from time-division multiplex-
format into frequency-division multiplex-format while retaining substantially
5 all phase and amplitude information of a band-limited continuous signal. This
document describes the use of the well-known multiplication (M), convolution
(C), multiplication (M) and CMC algorithm to perform such transformations.
Furtheron, it is described that a Fourier Transformation of an analog signal
sequence can be performed either by the MCM algorithm under use of chirp
10 signals or the CMC algorithm with such signals. In this context also a
reference is given to Fourier transform processors based on Surface Acoustic
Wave filters.

Furtheron, a description given by the Phonon Corporation discloses to assem-
15 ble spectrum analyzers and Fourier transformers from sets of dispersive delay
lines to perform a scanning for determining on which frequencies signals are
present. This description discloses that applications of such systems are also
advanced communication techniques, since they can process in real time at
rates far in excess of current digital techniques, with relatively little size,
20 weight and power.

The mathematical foundations for the MCM operation is shown in the
following. Under consideration of the Fourier Transformation $S(f)$ of a signal
 $s(t)$ which is bandlimited to B_e and of a maximum duration T_e , the Fourier
25 Transformation integral can be written in the form of the "chirp transform
algorithm":

$$S(f) = S(-a \cdot t) = ((s(t) \cdot Re(t)) * Rc(t)) \cdot Re(t),$$

Operation: M C M

30 where \cdot is multiplication, $*$ is convolution, $a = B_e/T_e$ is a scale factor, $Re(t)$ is a
chirp signal with the chirp rate $-a = -B_e/T_e$ and $Rc(t)$ is the impulse response
of an entity providing analog convolution with a length $T_c = 2T_e$ and a chirp
rate $a = B_c/T_c$.

35 However, no realization of a telecommunication device, e. g. an OFDM receiver
as shown in Fig. 8a, using such analog Fourier transformers for modulation
and/or demodulation purposes is known.

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1 Therefore, it is the object underlying the present invention to provide an improved OFDM telecommunication device that can cope with high bandwidth, but has an uncomplicated realization.

5 This object of the present invention is solved by an OFDM telecommunication device according to independent claim 1. Preferred embodiments thereof are respectively defined in the dependent subclaims.

10 An OFDM telecommunication device which comprises an analog RF and IF stage and a digital stage to output the baseband signal according to the present invention is characterized by a transformation unit that incorporates at least an analog multiplication step and at least an analog convolution step of a multiplication convolution multiplication algorithm or a convolution multi-
15 modulation convolution algorithm to perform a Fourier Transformation for de-modulation and/or an Inverse Fourier Transformation for modulation into the analog stage.

20 Therefore, according to the present invention not the whole MCM or CMC algorithm as shown in the prior art is incorporated into the FFT or IFFT block of a state of the art receiver or transmitter, but the Fourier Transformation or Inverse Fourier Transformation is performed distributed over several device entities. This arrangement has the advantage that several operations necessary within the state of the art telecommunication device can be adapted to perform there usual functionality as well as parts of the MCM or CMC algorithm. In
25 particular, both multiplication steps of the MCM algorithm can be combined with the RF/IF up- or down-conversion and the modulation or demodulation, i.e. the IQ modulation or demodulation. Therefore, the transformation unit according to the present invention is preferably arranged in the lowest IF-stage.

30 Another advantage is that in case of the MCM algorithm only those processing steps that require high bandwidth, i. e. the up- or down-conversion multiplication step and the convolution step, are necessarily performed with analog devices and the IQ modulation or demodulation step can be performed in the digital stage if this is desired.

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Furtheron, in case of a transceiver which incorporates the MCM algorithm, the same analog convolution and multiplication device can be used for receiving

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1 and transmitting, but only the sign of the slope of the chirp functions has to be changed for the different functionality, since all OFDM-systems are time multiplex semi duplex systems.

5 Still furtheron, according to the present invention, a correlator used to perform the FFT can also be used to perform the OFDM time synchronization.

The present invention and its objects, features and advantages will be better understood from the following description of exemplary embodiments thereof
10 taken in conjunction with the accompanying drawings, wherein

Fig. 1 shows an OFDM telecommunication device according to the present invention;

15 **Fig. 2** shows the schematic signal flow for the analog Fourier Transformation used within the telecommunication device shown in Fig. 1;

Fig. 3 shows the schematic signal flow for the Fourier Transformation of subsequent OFDM symbols within the telecommunication device shown in Fig. 1;
20

Figs. 4a and 4b show block diagrams of an OFDM receiver and an OFDM transmitter according to a first further preferred embodiment of the present invention;
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Figs. 5a and 5b show block diagrams of an OFDM receiver and an OFDM transmitter according to a second further preferred embodiment of the present invention;
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Figs. 6 a and 6b show block diagrams of an OFDM receiver and an OFDM transmitter according to a third further preferred embodiment of the invention;

35 **Figs. 7a and 7b** show block diagrams of an OFDM receiver and an OFDM transmitter according to a fourth further preferred embodiment of the present invention;

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- 1 **Figs. 8a and 8b** show a receiver according to the prior art in comparison to a receiver according to an embodiment of the present invention; and
- 5 **Fig. 9** shows the (simulated) spectrum of an OFDM signal demodulated according to the present invention.

The advantageous exemplary embodiments show only an incorporation of the MCM algorithm, since its implementation offers more flexibility. On the other hand, the present invention is not limited thereto and those skilled in the art are aware of the modifications necessary to implement the CMC algorithm.

Fig. 1 shows an OFDM telecommunication device 1 that is connected via a data bus 4 to a data processor 5. The telecommunication device 1 comprises an antenna 3 and a transformation unit 2 according to the present invention which provides an at least partly analog FT/IFT processing function.

The telecommunication device 1 can be either a receiver receiving OFDM-signals via the antenna 3 and outputting data signals calculated with the help of the at least partly analog Fourier Transformation by a receiver transformation unit 2a to the data processor 5 via the data bus 4, a transmitter receiving data signals from the data processor 5 via the data bus 4 and generating OFDM-signals to be output via the antenna 3 on basis of the at least partly analog calculated Inverse Fourier Transformation by a transmitter transformation unit 2b, or a transceiver combining these both functions.

An analog FT/IFT function in this context means that in case of a transmitter at least the convolution and the following multiplication of the MCM algorithm are calculated with analog means, i. e. the transmitter transformation unit 2b comprises an input stage with an analog delay means having different delay properties, such as a specially designed surface acoustic wave device or a charge coupled device, followed by an analog multiplier as output stage which additionally receives a corresponding chirp signal to multiply the output signal of the analog delay means with. The preceding multiplication can e. g. also be performed within the transmitter transformation unit 2b or within an IQ processing stage that is arranged preceding to the transmitter transformation unit 2b. In case of a receiver, on the other hand, at least the convolution and the preceding multiplication is conducted by analog means, i. e. the receiver trans-

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1 formation unit 2a comprises an input stage with an analog multiplier to multiply the input signal with a chirp signal, followed by an analog delay means having corresponding different delay properties, such as a surface acoustic wave filter or a charge-coupled device. The following multiplication can e. g.
5 also be performed within the receiver transformation unit 2a or within an IQ processing stage following the receiver transformation unit 2a.

The respective other multiplication necessary for conducting the MCM algorithm, i. e. the preceding multiplication in case of a transmitter and the following multiplication in case of a receiver, can either be conducted analogically
10 or digitally.

Fig. 2 shows the schematic signal flow for the analog Fourier Transformation using the MCM algorithm, i. e. the schematic signal flow from the multiplication with following convolution conducted within an OFDM receiver
15 according to the present invention.

The left-hand side of the time frequency graph shows the expanded signal as it appears at the compressor input which contains a lowest frequency f_1 and a
20 highest frequency f_2 with a chirp signal $Re(t)$ with a chirp rate $-a = -B_e/T_e$ wherein B_e is the bandwidth, i. e. $f_2 - f_1$, and T_e is the length of one OFDM symbol. Exemplary shown are the two cases of a multiplication of f_1 with the chirp signal and f_2 with the chirp signal. The resulted chirp signal has the resulted center frequency f_e . Therefore, the left hand side of the time frequency
25 graph shows the shifting of f_e by an upper input frequency f_2 and a lower input frequency f_1 .

Preferrably, within this step the down-conversion of the radio frequency to the lowest intermediate frequency stage is performed. In this case the demodulator
30 102 as described and shown in connection with Fig. 8a can be omitted. Instead, an OFDM receiver according to the present invention which can be compared to the OFDM receiver according to the prior art shown in Fig. 8a comprises a multiplier 110 that receives a first chirp signal which is provided by a first chirp generator 109, as shown in Fig. 8b. This multiplier 110 per-
35 forms the first multiplication of the MCM algorithm and preferrably simultaneously the down-conversion of the RF signal to the IF signal. To simultaneously perform the down conversion, the center frequency of the chirp

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- 1 signal must correspond to the respective incoming frequency range, i. e. RF or IF.

The chirp signal can be the impulse response of a device having different propagation delay properties like a surface acoustic wave chirp filter or a signal which is generated by a chirp generator 109, as it is shown in Fig. 8b. The chirp generator 109 can generate the chirp signal in an analog or digital manner.

- 10 The right-hand side of the time frequency graph shown in Fig. 2 shows the compression, i. e. the convolution of the multiplied RF-signal with the impulse response $R_c(t)$ of an analog delay means having different delay properties. Such a delay means has different propagation delays for different frequencies and can be e. g. a SAW (Surface Acoustic Wave) chirp filter or a special CCD (Charge-Coupled Device). The impulse response is of a length $T_c = 2T_e$ and a chirp rate $a = B_c/T_c$.

Preferrably, the operation is done in the IF stage with center frequencies between 100 MHz and 1 GHz and bandwidths of 20 - 100 MHz.

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- For the example shown at the left hand side of the time frequency graph, the right hand side of said graph shows one sloped line indicating the points of time of appearance of the respective signal in the time domain. In the shown case the frequency $f_1 + f_e$ determines a point of time T_1 and the frequency $f_2 + f_e$ determines a point of time T_2 . At each of said points of time T_1 and T_2 a correlation peak is output as it is indicated on the lower right hand side of Fig. 2. Dashed peaks inbetween said both correlation peaks at T_1 and T_2 are caused by possible input frequencies between f_1 and f_2 . The shown frequency resolution $= 1/T_e$ is determined by the correlator.

30

In the embodiment of the present invention shown in Fig. 8b, this convolution step of the MCM algorithm is performed with a SAW convolver 111 that receives the output signal of the multiplier 110. In this embodiment the multiplier 110 and the SAW convolver 111 build the receiver transformation unit 2a.

- 35 The further signal processing can be performed in the digital way. Therefore, the output signal of the SAW filter 111 is input to an analog-to-digital converter 106 before a digital processor and IQ demodulator 112 further processes the signals and outputs them as digital inphase and quadrature sig-

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1 nals I and Q to a demapper 108 which outputs the baseband signal.

Of course, at least some steps of the further signal processing can also be performed in the analog way, e. g. the last multiplication of the MCM algorithm
5 and the IQ generation which can also be combined, as will be explained lateron. The analog way inherits the advantage to handle a higher bandwidth (estimated > 60 MHz) in comparison to the digital way according which allows a higher flexibility at moderate bandwidth (estimated < 60 MHz).

10 In the embodiment of the present invention shown in Fig. 8b the digital processor and IQ demodulator 112 supplies a control signal to the first chirp generator 109 via a digital-to-analog converter 113 which indicates to the first chirp generator 109 at which time a generated first chirp signal should begin and how this first chirp signal should look like.

15 Fig. 8b shows that according to the present invention the output signal of the surface acoustic wave convolver 111 is input to a digital processor and IQ demodulator 112 via an analog-to-digital converter 106. The analog-to-digital converter 106 also performs the IF to baseband conversion on basis of an undersampling. The digital processor and IQ demodulator 112 multiplies the resulting signal with a second chirp signal $Re(t)$ at a chirp rate $-a = -B_e/T_e$. The
20 second chirp signal is generated within the digital processor and IQ demodulator 112 itself. Furtheron, the separation of the amplitude and phase information is performed using a 90° phase splitter for $Re(t)$ similar to common IQ
25 modulators.

Of course, depending on the wanted implementation the last multiplication of the MCM algorithm and the IQ demodulation can also be performed within the analog stage whereafter the resulting inphase and quadrature signals will be
30 supplied to the demapper 108 via an analog-to digital converter.

However, as mentioned above, according to the present invention a combination of the IQ demodulation and the last multiplication of the MCM algorithm is advantageously performed. This can be done by a multiplication of the output signal of the delay means with the inphase component of the second chirp
35 signal $Re(t)$ to obtain the inphase component of the complex spectrum of the demodulated OFDM signal as well as a multiplication of the output signal of the delay means with the quadrature component of the second chirp signal

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1 Re(t) to obtain the quadrature component of the complex spectrum of the de-
modulated OFDM signal. Such multiplications can be performed within the
analog stage or within the digital stage with a chirp signal that is analogically
generated or that is digitally generated. Of course, the IQ demodulation can be
5 performed with all generally known algorithms or methods.

Using the Fourier Transformation algorithm described above a fast execution of
the Fourier Transformation of subsequent following OFDM symbols can be real-
ized.

10 The processing of subsequent following OFDM symbols according to the
present invention is shown in Fig. 3. Two subsequent symbols are separated by
a guard interval. The Fourier Transformation of the first symbol is performed
in the shown FT window without disturbance by the following symbol.

15 The upper part of Fig. 3 shows that first the output signals from the expander
are fed into the compressor. This part of the diagram is similar to Fig. 2. The
output signals of the expander are shown as lowest chirp and highest chirp.
Of course, a number of different chirps can be in-between those both shown
20 chirps.

The middle part of Fig. 3 shows that the lowest chirp, i. e. the chirp of the low-
est frequency, from the expander which is completely fed into the compressor
causes the first output signal peak at the time T1. The highest chirp, i. e. the
25 chirp of the highest frequency, or a chirp lying in-between the lowest and high-
est chirps does not produce an output signal at T1.

The lower part of Fig. 3 shows that the highest chirp signal which is completely
fed into the compressor generates an output signal at the time T2. The time in-
30 between T1 and T2 corresponds to the FT window. All chirps lying in-between
the lowest and highest chirps produce output signals in-between T1 and T2.
The lowest frequency chirp or a chirp lying in-between the lowest and highest
chirps does not generate a signal at T2. Also, the following lowest chirp signal
does not generate a signal at T1.

35 In the following four further preferred embodiments of the present invention
additionally to the embodiment shown in Fig. 8b are described. In the following
description of these further preferred embodiments the same, similar or corre-

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1 sponding elements are denoted with the same reference signs.

Fig. 4a shows a block diagram of an OFDM receiver according to a first further preferred embodiment of the present invention. The incoming IF-signal from the (not shown) front-end module of the OFDM receiver is input to a multiplier 6 that multiplies this IF-signal with a first chirp signal $Re(t)$ generated by a first chirp generator 10b. If it is desired, this multiplier 6 can simultaneously perform the RF down-conversion to IF in case the front-end module outputs a RF-signal as described above.

10

The first chirp signal $Re(t)$ can be generated either by an analog or digital signal generator or using the impulse response of a chirp filter, e. g. a surface acoustic wave chirp filter or a charge-coupled device. The first chirp generator 10b receives time- and frequency-synchronisation signals according to which the first chirp signal $Re(t)$ is generated. Therefore, the chirp signal $Re(t)$ is controlled in start time and center frequency.

15

The output signal of the multiplier 6 is input to a convolver 7 which provides an analog convolution, e. g. a surface acoustic wave chirp filter or a charge-coupled device. The convolver 7 and the multiplier 6 together build the receiver transformation unit 2a which is incorporated into the analog stage of the OFDM receiver and which provides the first multiplication and the convolution of the MCM algorithm.

20

25 The output signal of the receiver transformation unit 2a is input to a second multiplier 8 which multiplies it with a second chirp signal $Re(t)$ and to a third multiplier 9 which multiplies it with said second chirp signal $Re(t)$ which is phase-shifted bei 90° . Therewith, each of said both multipliers 8 and 9 performs the last multiplication of the MCM algorithm to complete the Fourier Transformation. Simultaneously an IQ demodulation is performed, since amplitude and phase information of the complex spectrum of the demodulated OFDM signal are separated by using a 90° phase splitter for the second chirp signal $Re(t)$. Furtheron, also a down-conversion from the intermediate frequency to the baseband can be performed simultaneously, since the multiplication provides a lower and an upper sideband and the lower sideband is the baseband signal.

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The center frequencies of the first chirp signal generated by the first chirp gen-

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erator 10b for the signal expansion by the multiplier 6 and the second chirp signal generated by a second chirp generator 10a which is also used for the IQ demodulation can be different. Since all other parameters of these both chirp signals are equal, both of those signals are called $Re(t)$. In contrast to the first chirp generator 10b which receives time- and frequency-synchronisation signals, the second chirp generator 10a only receives a time synchronisation signal, since only the start of the chirp signal has to be controlled in this stage. The center frequency of the second chirp can be fixed. The frequency synchronization is only additionally necessary for controlling the center frequency of the first chirp signal.

The output signal of the second multiplier 8 is input to an analog-to-digital converter 15 via a low-pass filter 13 to be fed to the digital stage as real signal and the output signal of the third multiplier 9 is input to an analog-to-digital converter 16 via a low-pass filter 14 to be fed to the digital stage as imaginary signal. In case the down-conversion from IF to baseband is not performed simultaneously with the multiplication with the second chirp signal, such a down-conversion can advantageously be performed during the analog to digital conversion.

Fig. 4b shows a block diagram of a corresponding OFDM transmitter according to the first preferred embodiment of the present invention, i. e. an OFDM transmitter performing the MCM algorithm completely within the analog stage. Furtheron, the OFDM transmitter incorporates the IQ modulation as well as the baseband to IF up-conversion within the first multiplication step of the MCM algorithm and IF to IR up-conversion within the last multiplication step of the MCM algorithm.

The (not shown) digital stage of the shown OFDM transmitter provides real and imaginary input signals. The real input signal is supplied to a fifth multiplier 23 via a digital-to-analog converter 28 and a low-pass filter 26. The multiplier 23 multiplies the incoming signal with a second chirp signal $Re(t)$ generated by a second chirp generator 10a which generates said chirp signal based on a control signal. This control signal is directly comparable to the time synchronization signal used within the receiver and therefore cares for a synchronous processing (multiplication) of the OFDM signals with the chirp signals. The imaginary input signal is supplied to a sixth multiplier 24 via a digital-to-analog converter 29 and a low-pass filter 27. The sixth multiplier 24 multiplies

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- 1 the input signal with said second chirp signal $Re(t)$ which is phase-shifted by
90°. The output signals of said both multipliers 23 and 24 are input to an
adder 25 which adds them and inputs the resulting sum signal to a transmitter
transformation unit 2b which performs the convolution and second multiplica-
5 tion of the MCM algorithm in an analog manner.

The transformation unit 2b comprises an analog delay means 7 as input stage
and an analog multiplier 22 as output stage. The output signal of said analog
delay means 7 is input to the analog multiplier 22 which multiplies with a first
10 chirp signal $Re(t)$ generated by a first chirp generator 10b which also receives
the control signal supplied to the chirp generator 10a.

As mentioned above, the second and first chirp signals $Re(t)$ generated by the
second chirp generator 10a and by the first chirp generator 10b are identical
15 apart from their center frequencies which might be different. Both signals are
also identical to the chirp signals used in the receiver and have the same time
relationships.

The analog multiplier 22 might not only perform the last multiplication of the
20 MCM algorithm, but can simultaneously perform an up-conversion from the IF-
signal to the RF-signal to be transmitted via a (not shown) front-end module
similarly to the down-conversion advantageously performed within the re-
ceiver transformation unit 2a.

- 25 To perform the IFT within the transmitter the same MCM algorithm is used as
within the receiver, but chirp signals with a different slope are used, i. e. with
a slope having the inverse sign, whereas the passive correlator can be the same
element, since the signal flow is inversed, i. e. the terminal serving as input in
case of a receiver serves as output in case of a transmitter and the terminal
30 serving as output in case of a receiver serves as input in case of a transmitter.

A block diagram of an OFDM receiver according to a second further preferred
embodiment of the present invention is shown in Fig. 5a. In contrast to the
OFDM receiver according to the first further preferred embodiment in which
35 the whole MCM algorithm is performed in the analog stage of the receiver, ac-
cording to the second further preferred embodiment only parts of the MCM al-
gorithm are performed in the analog stage, namely the first multiplication and
the convolution.

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1 Therefore, the receiver transformation unit 2a is identical to and has the same
functionality as the receiver transformation unit 2a of the first further pre-
ferred embodiment. The output signal of the analog convolver 7 is input to a
digital processing unit 19 via an analog-to-digital converter 17. The digital
5 processing unit 19 additionally receives a time synchronisation signal and
based on its both input signals generates real and imaginary output signals.
The digital processing unit 19 performs the second multiplication of the MCM
algorithm, i. e. a multiplication of the output signal of the analog convolver 7
with a second chirp signal generated within the digital processing unit 19 and
10 the IQ generation. The IF-to-baseband-conversion is performed in the digital
processing unit 19.

According to this second further preferred embodiment the first chirp signal
 $Re(t)$ supplied to the first analog multiplier 6 is generated by a first digital
15 chirp generator 10c which receives the time synchronisation signal and a fre-
quency synchronisation signal. The first digital chirp generator 10c supplies
the first chirp signal to the first multiplier 6 via a digital-to-analog converter
18.

20 A corresponding OFDM transmitter according to the second preferred
embodiment of the present invention is shown in Fig. 5b.

Real and imaginary input signals are supplied to a digital processing unit 34
which performs the first multiplication of the MCM algorithm with a second
25 chirp signal $Re(t)$ generated within the digital unit 34 based on a control signal
input thereto. Furtheron, the digital processing unit 34 performs an up-con-
version to the first IF. The IF output signal of the digital processing unit 34 is
supplied to a transformation unit 2b via a digital-to-analog converter 30. Said
transmitter transformation unit 2b is identical to the transmitter transforma-
30 tion unit 2b of the first further preferred embodiment according to the present
invention.

Similar to the receiver according to the second further preferred embodiment
of the present invention shown in Fig. 5a also the OFDM transmitter according
35 to the second further preferred embodiment of the present invention shown in
Fig. 5b comprises a first digital chirp generator 10c that supplies the digitally
generated first chirp signal $Re(t)$ to the fourth multiplier 22 of the
transformation unit 2b via a digital-to-analog converter 31. The first digital

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- 1 chirp generator 10c generates the first chirp signal $Re(t)$ based on a control signal.

Fig. 6a shows a block diagram of an OFDM receiver according to a third further preferred embodiment of the present invention. This embodiment basically works similar to the OFDM receiver according to the second further preferred embodiment of the present invention shown in Fig. 5a, but the digital processing unit 19 within the digital stage that performs the second multiplication of the MCM algorithm and the IQ demodulation is exchanged with an IQ generator 21 directly after the analog-to-digital converter 17 that digitally generates the inphase and quadrature signals which are then input into a CORDIC block 20 that performs the second multiplication of the MCM algorithm on basis of the CORDIC algorithm and therefore outputs the real and imaginary signals of the complex spectrum of the demodulated OFDM signal. Therefore, said CORDIC block 20 also receives the time synchronisation signal similar to the digital processing unit 19 of the first further preferred embodiment.

The CORDIC algorithm is a very simple way to replace the complex multiplication in the IF stage with a phase rotation in the baseband which has the same effects. Therefore, the CORDIC algorithm replaces the respective multipliers and low pass filters shown in the first further preferred embodiment, since aliasing signals present in the baseband which have to be filtered out in the IF stage are simply discarded by the CORDIC algorithm.

A transmitter according to the third further preferred embodiment of the invention simply works in reversed mode, i. e. as it is shown in Fig. 6b, wherein the digital processing unit 34 of the second further preferred embodiment of the present invention, as it is shown in Fig. 5b, is replaced with a CORDIC block 20 adapted to perform the first multiplication with the second chirp signal of the MCM algorithm.

Fig. 7a shows a block diagram of an OFDM receiver according to a fourth further preferred embodiment of the present invention. According to this fourth further preferred embodiment the analog second multiplication of the MCM algorithm and the analog low-pass filtering as shown in Fig. 4a for the OFDM receiver according to the first further preferred embodiment of the present

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1 invention is shifted into the digital stage, i. e. the output signal of the receiver
transformation unit 2a is input to second and third multipliers 8 and 9 via an
analog-to-digital converter 17. In this fourth further preferred embodiment the
second and third multipliers 8 and 9 are realized as digital multipliers which
5 output their respective output signal to digital low-pass filters 13 and 14. Fur-
theron, the second chirp signal is digitally generated by a digital third chirp
generator 10c and input to a digital 90° phase splitter 11 which outputs the
digital second chirp signal $Re(t)$ to the second multiplier 8 and the 90° shifted
digital second chirp signal $Re(t)$ to the third multiplier 9. Furtheron, the digital
10 second chirp signal $Re(t)$ passes through a digital delay element 36 to be con-
verted into a digital first chirp signal and a digital-to-analog converter 18 to
the first analog multiplier 6 of the transformation unit 2a. The receiver trans-
formation unit 2a is identical to and has the same functionality as the receiver
transformation unit 2a shown and described in connection with the first fur-
15 ther preferred embodiment of the present invention. The digital third chirp
generator 10c generates digital chirp signals depending on time and frequency
synchronisation signals.

Corresponding thereto Fig. 7b shows the block diagram of an OFDM
20 transmitter according to the fourth further preferred embodiment of the
present invention. This OFDM transmitter basically works in reversed mode to
the OFDM receiver according to the fourth further preferred embodiment of the
present invention shown in Fig. 7a.

25 Therefore, real and imaginary input signals are supplied to fourth and fifth
multipliers 23 and 24, respectively via low-pass filters 32 and 33. The fourth
and fifth multipliers 23 and 24 as well as the low-pass filters 32 and 33 are re-
alized digitally. As in the first further preferred embodiment, the fourth and
fifth multipliers 23 and 24 perform the first multiplication of the MCM
30 algorithm i. e. a multiplication with a second chirp signal $Re(t)$. In this case
the second chirp signal $Re(t)$ is generated by the digital third chirp generator
10c and is supplied inphase to the multiplier 23 and in quadrature to the
multiplier 24 via a digital 90° phase splitter 11. The output signals of said
both multipliers 23 and 24 are input to a digital adder 25 which supplies the
35 resulting sum signal to the transmitter transformation device 2b via a digital-
to-analog converter 30. The transmitter transformation device 2b is identical
to and has the same functionality as the transmitter transformation device 2b

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1 shown and described in connection with the first further preferred embodiment
of the present invention. In contrast to this first further preferred embodiment
of the present invention the chirp signal needed for the second multiplication
step of the MCM algorithm which is performed by the analog multiplier 22 is
5 the same second digital chirp signal $Re(t)$ generated by the digital third chirp
generator 10c on basis of a control signal supplied thereto which passes
through a digital delay element 36 and a digital to analog converter 31.

As can be seen from the description of the preferred embodiments according to
10 the present invention, many modifications can be made without departing from
the general concept of the present invention to provide an analog transforma-
tion unit within the analog stage of an OFDM telecommunication device which
performs the main calculation needed for the Fourier Transformation or the In-
verse Fourier Transformation.

15 The present invention is particularly applicable to BRAN systems, which is
shown by the following simulation example.

The spectral resolution Δf is determined by the duration of the expander chirp
20 (T_e) to $\Delta f = 1/T_e$. Assuming a length of $T_e = 3.2 \mu\text{sec}$ the FT has a spectral
resolution of 312 kHz. Furthermore, the analytic bandwidth $B = a(B_c - B_e)$ ($|a|$
 $= B_c/T_c = B_e/T_e$). Assuming an expander bandwidth of 20 MHz the length of
the analytic bandwidth is 20 MHz.

25 The MCM FT algorithm has been applied on proposed device topology according
to the method of operation. Fig. 9 shows the spectrum of an OFDM signal de-
modulated by one of the receiver assemblies according to the present inven-
tion.

30 The applied simulation set-up, i. e. analyzed signal bandwidth: 20 MHz, $T_e =$
 $3.2 \mu\text{sec}$, $T_c = 6.4 \mu\text{sec}$, $B_e = 20 \text{ MHz}$, $B_c = 40 \text{ MHz}$, $\Delta f = 312 \text{ kHz}$, 64 point
analog FT, 48 carriers used, is similar to the high data rate wireless LAN sys-
tem called HIPERLAN/2, which is currently under standardization.